



Design of 2x2 MIMO OFDM Architecture for Fixed WIMAX

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Abstract- Multiple Input Multiple Output Orthogonal Frequency Division Multiplexing technology is an advanced transmission technique for wireless communication systems. In this paper, the 64 point pipeline FFT/IFFT processor is introduced for efficient implementation of OFDM architecture. The IFFT processor is used to modulate the subcarrier in transmitter section and FFT processor demodulate the subcarrier in receiver section in the architecture. Our design adopts a single-path delay feedback style requiring less memory space and reconfigurable complex constant multiplier and bit parallel multiplier used in pipeline FFT/IFFT processor, instead of using ROM's to store twiddle factors that consuming lower power. The design of ROM-less FFT/IFFT processor is applied to OFDM architecture with different encoding and decoding techniques analysis in the IEEE 802.16d communication standard. The result shows overall architecture design using the ROM-less FFT/IFFT processor with convolutional encoding and decoding gives efficient power, area and timing specifications considerably.

Keywords-MIMO, OFDM, FFT, IFFT.

I. INTRODUCTION

The rapid growth of digital communication in recent years, which need for high-speed data transmission, has been increased. The mobile telecommunications industry faces the problem of providing the technology that be able to support a variety of services ranging from voice communication with a bit rate of a few kbps to wireless multimedia in which bit rate up to 2 Mbps. Many systems have been proposed and OFDM system has gained much attention for different reasons. Although OFDM was first developed in the 1960s, only in recent years, it has been recognized as an outstanding method for high-speed cellular data communication where its implementation relies on very high-speed digital signal processing. This method has only recently become available with reasonable prices versus performance of hardware implementation.

Generally, the pipeline FFT processors have two popular design types. One uses single-path delay feedback (SDF) pipeline architecture and the other uses multiple-path delay commutator (MDC) pipeline architecture. The single-path delay feedback (SDF) pipeline FFT is good in its requiring less memory space (about $N-1$ delay elements) and its multiplication computation utilization being less than 50%, as well as its control unit being easy to design. Such implementations are advantageous to low-power design, especially for applications in portable DSP devices. Based on these reasons, the SDF pipeline FFT is adopted in our work. However, the FFT computation often needs to multiply input signals with different twiddle factors for an outcome, which results in higher hardware cost because a large size of ROM is needed to store the wanted twiddle factors. Therefore, to throw off these ROM's for area-efficient consideration, Mao-Hsu Yen, have proposed an efficient ROM-less FFT/IFFT processor. The complex multipliers used in the processor are realized with shift-and-add operations. Hence, the processor uses only a two-input digital multiplier and does not need any ROM for internal storage of coefficients. However, low speed and higher hardware cost caused by the proposed complex multiplier are the pay-off.

Chu Yu and Mao-Hsu Yen have proposed the design of Low-Power 64-point Pipeline FFT/IFFT Processor for OFDM Applications. This design adopts a single-path delay feedback style as the proposed hardware architecture to eliminate the read-only memories (ROM's) used to store the twiddle factors. R.Premalatha and M.Shanthi has proposed the design of 2x2 MIMO-OFDM System on FPGA. FPGA implementation is carried with good channel estimation method, efficient FFT/IFFT processor and better coding techniques. In MIMO-OFDM systems, the information bits are carried by the transmitter and receiver section. Here transmitter contains scrambler, encoder, interleaver, modulation, IFFT processor, pilot insertion, adding cyclic prefix and preamble then convert into the RF frequency to the antenna. The reverse operation is performed in the receiver section. In order to reduce the area and power consumption in the FFT processor, the overall architecture chip area is minimized. That will give the efficient OFDM architecture for reliable data transmission.

This paper is organized as follows. In section II, the system block diagram of the MIMO-OFDM is shown, which presents each block design explanation in the OFDM systems including the proposed pipeline FFT/IFFT processor for application in wireless communication systems. In section III, Simulation results, area and power report analysis. Finally, Conclusions are in section IV.

II. OFDM ARCHITECTURE

The architecture of the transmitter and receiver is illustrated in Figure 1 and Figure 2 respectively [2], [3]. The bit stream which has been scrambled and interleaved is separated into spatial streams by stream parser. Then the spatial streams are mapped into constellation. The points on the constellation are through the STBC encoder to transform the spatial streams to space-time streams. After that spatial mapper maps space-time streams into transmit chains. And the transmit chains are inserted pilot IFFT modulated, added CP (Cyclic Prefix), then transmitted through the RF modules. The transmitted signals are received through RF modules and remove CP. The received chains are FFT modulated, pilot extraction, channel estimation and passed through the STBC decoder to transform to spatial streams from space-time stream. The spatial streams are demapped, interleaved, and descrambled to get the original bit stream.

A. Scrambler and Descrambler

A scrambler is a device that describes randomizes the data stream to remove repeated patterns. In the transmitter, a pseudorandom cipher sequence is added to the data sequence to produce a scrambled data sequence. [4] The pseudorandom cipher sequence is described by the generating polynomial $G(x) = X^{11} + X^9 + 1$. In the receiver, the same pseudorandom cipher sequence is subtracted from the scrambled data sequence to recover the transmitted data sequence. The information bits are randomized before the transmission. The randomizer, which is the first block in the transmitter, performs randomization of input data on each burst on each allocation to prevent a long sequence of 1's and 0's. This is implemented by using a Pseudo Random Binary Sequence (PRBS) generator. By using descrambler section the data sequence is retrieved from the scrambled data by reversing the operation.

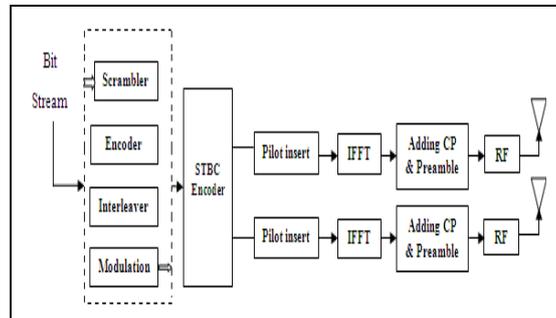


Figure 1. OFDM Architecture of the Transmitter

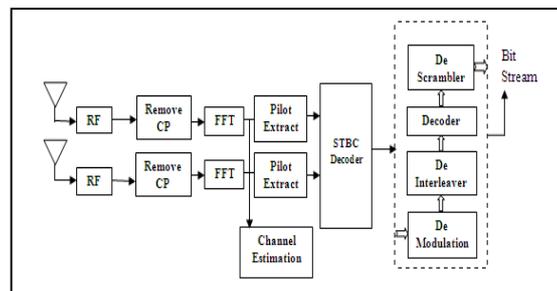


Figure 2. OFDM Architecture of the Receiver

B. Interleaver and Deinterleaver

Interleaving is frequently used in digital communication and storage systems to improve the performance of forward error correcting codes. Many communication channels are not memoryless errors typically occur in bursts rather than independently. If the number of errors within a code word exceeds the error-correcting code's capability, it fails to recover the original code word. Interleaving ameliorates this problem by shuffling source symbols across several code words, thereby creating a more uniform distribution of errors. The deinterleaving gives reverse shuffling operation of transmitted signals.

C. Modulation and Demodulation

The Modulator passes interleaved data through a serial to parallel converter, mapping groups of bits to separate carriers, and encoding each bit group by frequency, amplitude, and phase. The QPSK is a phase modulation scheme, used in constellation mapping [6]. The constellation map of QPSK modulator is shown in Figure 3. Here the input bits stream is converted into complex stream using equation (1) and where I and Q both are in phase with I-out and Q-out respectively are shown in table I. QPSK modulator accepts the binary bits as inputs consider as a symbol and

converts them into complex value. QPSK takes only 4 symbols and generate its complex value in this fashion because the bit rate is $\frac{1}{2}$.

$$D = (I + jQ) * KMOD \text{ where } KMOD = 1/1.414 \tag{1}$$

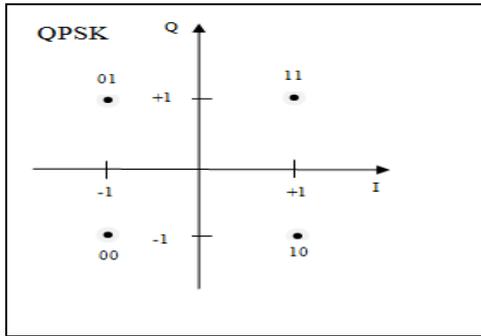


Figure 3. QPSK Constellation Mapping

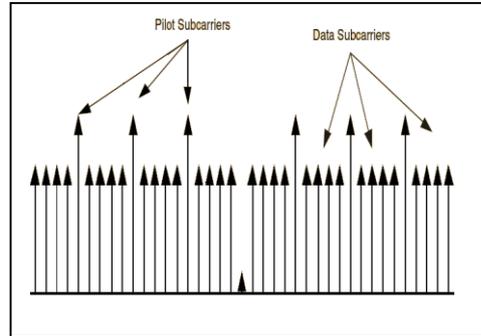


Figure 4. Pilot insertion in Subcarriers

TABLE I INPUTS AND OUTPUTS OF QPSK MODULATOR

Input Bits	I out	Q out
00	-1	-1
01	-1	+1
10	+1	-1
11	+1	+1

D. STBC Encoder

Space time block coding is a technique used in wireless communications to transmit multiple copies of a data stream across a number of antennas and to exploit the various received versions of the data to improve the reliability of data-transfer. Alamouti’s transmit diversity scheme with two transmit antennas and two receive antennas are used. [10] Alamouti’s scheme is a space-time block code and suitable when two transmit antennas and an arbitrary number of receive antennas are used.

E. Pilot Insertion

Pilot insertion adds the values for pilot and guard subcarriers to OFDM symbols. A transmitting entity transmits a “base” pilot in each protocol data unit (PDU). A receiving entity is able to derive a sufficiently accurate channel response estimate of a MIMO channel with the base pilot under nominal (or most) channel conditions. The transmitting entity selectively transmits an additional pilot if and as needed, e.g. (Figure 4), based on channel conditions and/or other factors. The additional pilot may be adaptively inserted in almost any symbol period in the PDU. The receiving entity is able to derive an improved channel response estimate with the additional pilot. The transmitting entity sends signaling to indicate that additional pilot is being sent. [5] This signaling may be embedded within pilot symbols sent on a set of pilot sub bands used for a carrier pilot that is transmitted across most of the PDU. The signaling indicates whether additional pilot is being sent and possibly other pertinent information.

F. Cyclic Prefix and Preamble

The cyclic prefix refers to the prefixing of data with a repetition of the end. As a guard interval, it eliminates the inter symbol interference from the previous data. It allows the linear convolution of a frequency-selective multipath channel to be modeled as circular convolution, which in turn may be transformed to the frequency domain using FFT. This approach allows for simple frequency-domain processing, such as channel estimation and equalization. [10] Preamble is used for synchronization and channel estimation at the receiver.

G. FFT/IFFT Processor

a) Rom-Less FFT/IFFT Processor

Traditional hardware implementation of FFT/IFFT processors usually employs a ROM to look up the wanted twiddle factors, and then word length complex multipliers to perform FFT computing. However, this introduces more hardware cost, thus a bit-parallel complex constant multiplication scheme is used to improve the foregoing issue. Besides, since the twiddle factors have a symmetric property. The complex multiplications used in FFT computation is one of the following three operation types [1]:

$$\text{Type1: } W_N^k \cdot (a + jb) = W_N^{k-(N/4)} \cdot (b - ja), \quad N/4 < k < N/2, \tag{2}$$

$$\text{Type2: } W_N^k \cdot (a + jb) = -W_N^{k-(N/2)} \cdot (b - ja), \quad N/2 < k < 3N/4, \tag{3}$$

$$\text{Type3: } W_N^k \cdot (a + jb) = -W_N^{k-(3N/4)} \cdot (b - ja), \quad 3N/4 < k < N, \quad (4)$$

Any twiddle factor can be obtained by a combination of these twiddle-factor primary elements. In other words, arbitrary twiddle factor used in FFT can utilize these operation types to derive the wanted value, thus can significantly shorten the size of ROM used to store the twiddle factors. Moreover, for hardware implementation consideration, we add two extra operation types to further decrease the size of ROM. Our method can also run away the critical path in the designed hardware such that the system clock becomes faster compared to [7]-[9]. The two additional operation types are given by:

$$\text{Type 4: } W_N^k \cdot (a + jb) = \left[W_N^{(N/4)-k} \cdot (b + ja) \right], \quad 1 \leq k < N/4, \quad (5)$$

$$\text{Type 5: } W_N^k \cdot (a + jb) = -j \cdot \left[W_N^{(N/2)-k} \cdot (b + ja) \right], \quad N/4 < K < N/2, \quad (6)$$

A radix-2 64-point pipeline FFT/IFFT processor with low power consumption, as shown in Figure 5. [1], [3] The proposed architecture is composed of three different types of processing elements (PEs), a complex constant multiplier, delay-line (DL) buffers, and some extra processing units for computing IFFT. Here, the conjugate for extra processing units is easy to implement, which only takes the 2's complement of the imaginary part of a complex value.

b) Processing Elements

Based on the radix-2 FFT algorithm, the three types of processing elements (PE3, PE2, and PE1) used in our design are illustrated in Figure 6, Figure 7, and Figure 8, respectively. The functions of these three PE types correspond to each of the butterfly stages as shown in Figure 5. First, the PE3 stage is used to implement a simple radix-2 butterfly structure only, and serves as the sub modules of the PE2 and PE1 stages.

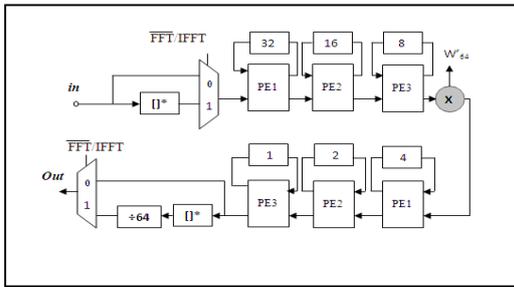


Figure 5. PE Types to Each of the Butterfly Stages

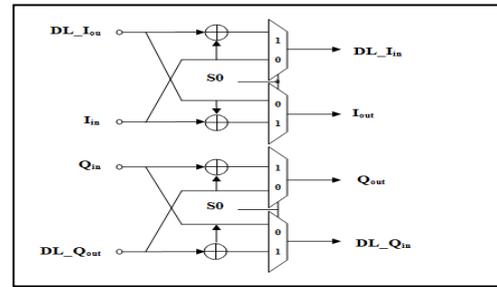


Figure 6. Circuit Diagram of PE3 Stage

In the Figure 6, Iin and Iout are the real parts of the input and output data, respectively. Qin and Qout denote the image parts of the input and output data, respectively. Similarly, DL_Iin and DL_Iout stand for the real parts of input and output of the DL buffers, and DL_Qin and DL_Qout are for the image parts, respectively.

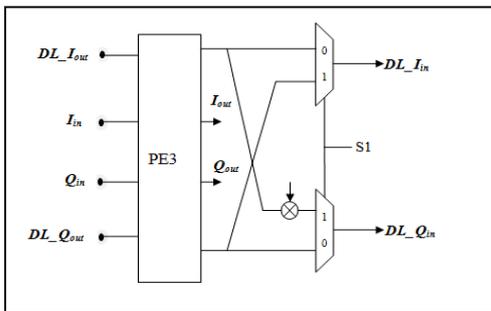


Figure 7. Circuit Diagram of PE2 Stage

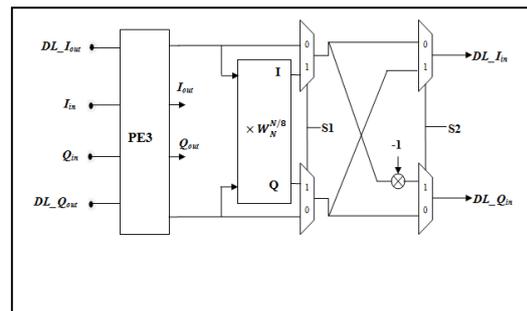


Figure 8. Circuit diagram of our proposed PE1 stage

As for the PE2 stage, it is required to compute the multiplication by $-j$ or 1 . Note that the multiplication by -1 in figure 5 is practically to take the 2's complement of its input value. In the PE1 stage, the calculation is more complex than the PE2 stage, which is responsible for computing the multiplications by $-j$, $W_N^{N/8}$, and $W_N^{3N/8}$, respectively.

Since $W_N^{3N/8} = -j W_N^{N/8}$, it can be given by either the multiplication by $W_N^{N/8}$ first and then the multiplication by $-j$ or the reverse of the previous calculation. Hence, the designed hardware utilizes this kind of cascaded calculation and multiplexers to realize all the necessary calculations of the PE1 stage. This manner can also save a bit-parallel multiplier for computing $W_N^{3N/8}$, which further forms a low-cost hardware.

c) *Bit-Parallel Multipliers*

In this section the multiplication by $1/2$ can employ a bit parallel multiplier to replace the word length multiplier and square root evaluation for chip area reduction.

$$\text{Output} = \text{in} \times \frac{\sqrt{2}}{2} = \text{in} \times (2^{-1} + 2^{-3} + 2^{-4} + 2^{-6} + 2^{-8} + 2^{-14}) \tag{7}$$

If a straightforward implementation for the above equation is adopted, it will introduce a poor precision due to the truncation error, and will spend more hardware cost. Therefore, to improve the precision and hardware cost, Eq. (7) can be rewritten as:

$$\text{Output} = \text{in} \times \frac{\sqrt{2}}{2} = \text{in} \times [1 + (1 + 2^{-2})(2^{-6} + 2^{-2})] \tag{8}$$

According to (8), the circuit diagram of the bit-parallel multiplier is illustrated in figure 9. The resulting circuit uses three additions and three barrel shift operations. The realization of complex multiplication by WNN/8 using a radix-2 butterfly structure with its both outputs commonly multiplied by $1/\sqrt{2}$ is shown in Figure 10. This circuit has just been used in the PE1 stage.

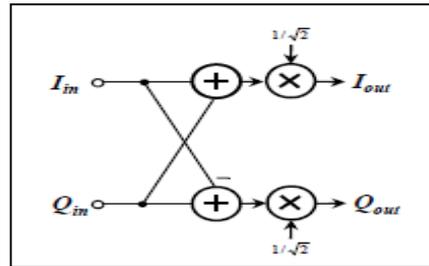
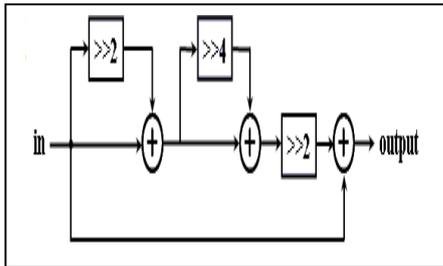


Figure 9. Circuit diagram of the Bit-Parallel Multiplication by $1/\sqrt{2}$ Figure 10. Circuit diagram of the multiplication by $W_N^{N/8}$

d) *Reconfigurable Complex Constant Multipliers*

A reconfigurable complex constant multiplier for computing W_{i64} is proposed, as shown in Figure 9 and Figure 10. This structure of this complex multiplier also adopts a cascaded scheme to achieve low-cost hardware. Here, the meaning of two input signals (I_{in} and I_{out}) and two output signals (Q_{in} and Q_{out}) are the same as the signals in the PE1 stage. In Figure 11, this circuit is responsible for the computation of multiplication by a twiddle factor W_{i64} , which is also an important circuit of our FFT/IFFT processor. The word length multiplier used in Figure 12 adopts a low-error fixed width modified Booth multiplier for hardware cost reduction.

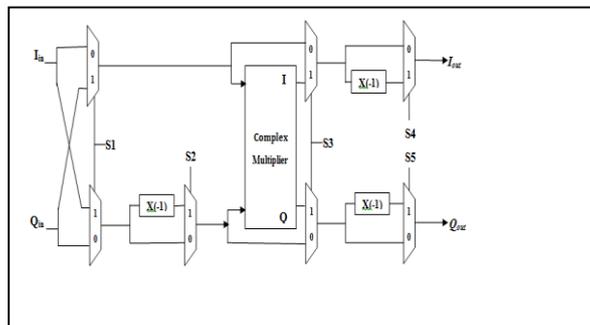


Figure 11. Proposed Reconfigurable Complex Constant Multiplier

The coefficient values $i1-i8$ and $q1-q8$ are listed in Table I, which can be used to synthesize the entire twiddle factors required in our proposed 64-point FFT processor. Besides, we need not to use bit-parallel multipliers to replace the word length one for two reasons. One is on the operation rate.

If bit-parallel multipliers are used, the clock rate is decreased due to the many cascaded adders. The other reason is the introduction of high wiring complexity because many bit-parallel multipliers are required to be switched for performing multiplication operations with different twiddle factors. Besides, we need not to use bit-parallel multipliers to replace the word length one for two reasons. One is on the operation rate. If bit-parallel multipliers are used, the clock rate is decreased due to the many cascaded adders.

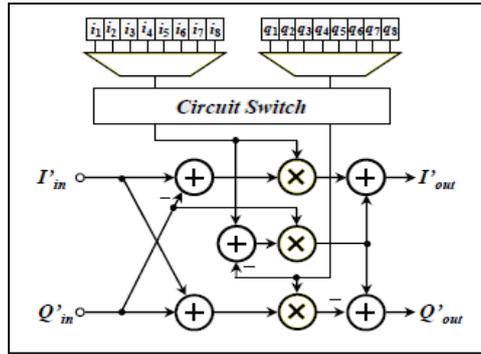


Figure 12. Block Diagram for Hamming Encoder

H. Analysis of Encoding and Decoding Techniques

When data is transmitted from one location to another there is always the possibility that an error may occur. There are a number of reliable codes that can be used to encode data so that the error can be detected and corrected. By using decoding techniques the redundant information to detect and correct errors occurred during transmission.

a) Hamming Encoding and Decoding

A Hamming Code can be used to detect and correct one bit change in an encoded code word. The block diagram is shown in Figure 13 where H[0]-H[3] are the original information bits and H[4]- H[7] are the parity bits.[12]. This approach can be useful as a change in a single bit is more probable than a change in two bits or more bits. The 8 bits output from the deinterleaving block are fed into the Hamming decoder in parallel shown in Figure 14. The counter controls MUX1 to select 4 out of 8 input data bits to perform the XOR operation. According to the properties of the (8, 4) Hamming coding, 5 XOR operations with different sets of input are necessary to perform error checking. After all the five different XOR operations is done, the XOR result is fed into the error checking module. At the same time, the 4 bits LSB of the input codewords and their inversions are ready at the input of MUX2. According to the XOR results, the error checking module decides whether there are errors in the received signal bits and indicates to MUX2 which output bit needs to be flipped. Finally, the correct 4-bit information codewords are selected and fed into the RXFIFO.

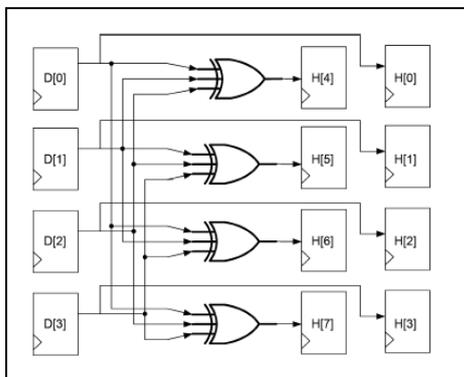


Figure 13. Block Diagram for Hamming Encoder

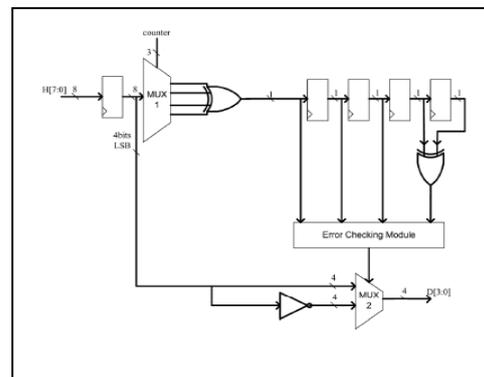


Figure 14. Block diagram of Hamming decoder.

b) Convolutional Encoding and Viterbi Decoding

A convolutional code introduces redundant bits into the data stream through the use of linear shift registers. The information bits are input into shift registers and the output encoded bits are obtained by modulo-2 addition of the input information bits and the contents of the shift registers. The block diagram is shown in Figure 15.

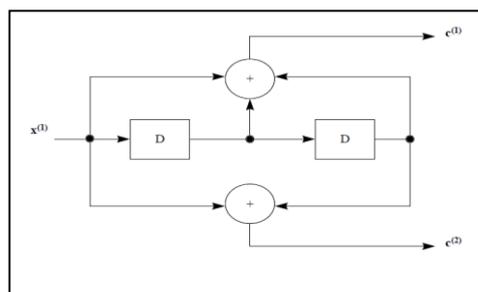


Figure 15. Block Diagram of Convolutional Encoder

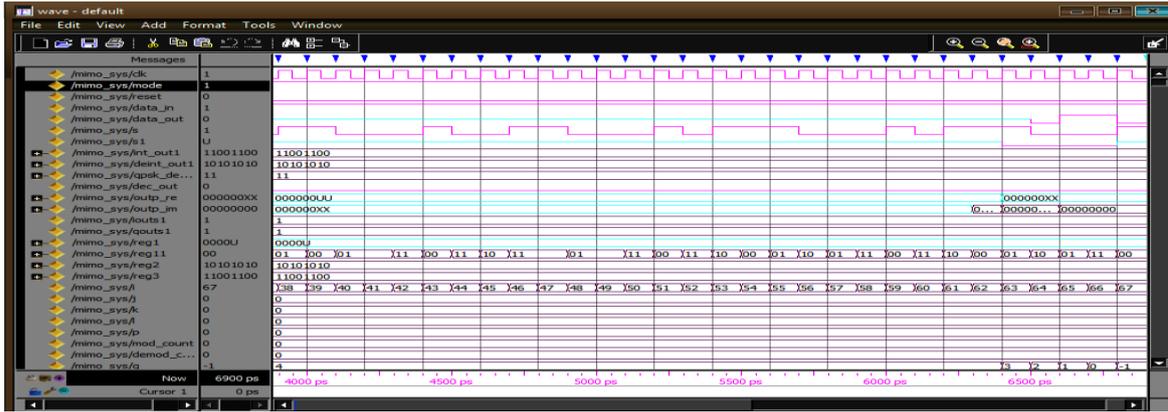


Figure 18. Simulation result of MIMO OFDM architecture using Convolutional Encoder and Viterbi Decoder

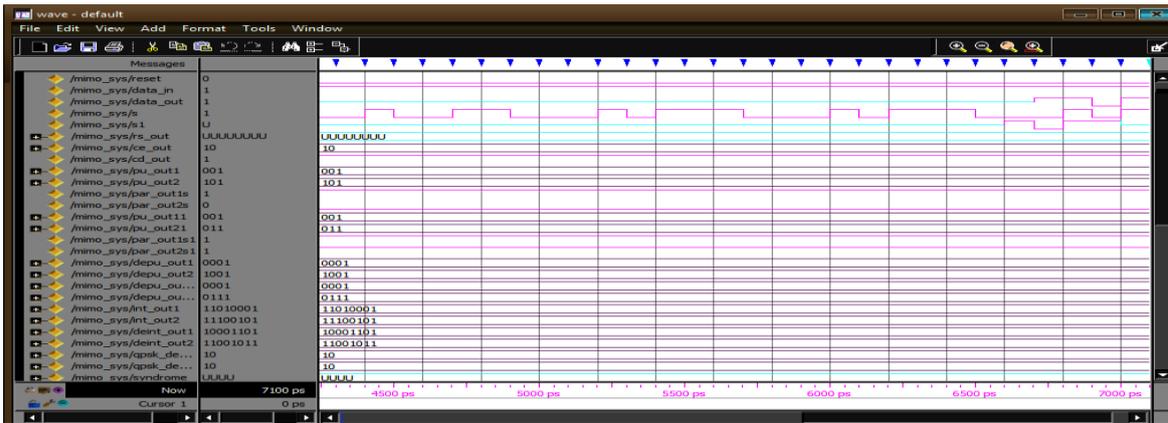


Figure 19. Simulation result of MIMO OFDM architecture using Convolutional Encoder and Sequential Decoder

A. Power and Area Report Analysis

The power and area analysis were done in Synopsys EDA tool and was found that for OFDM architecture, the total dynamic power and area specifications were met. The below shown result describes the power and area analysis and the result was found that for an OFDM architecture using Synopsys Design Compiler tool. The Table II describes the detailed comparison of area utilization and power consumption of FFT/IFFT processor design and the Table III describes the detailed area utilization and power consumption for different coding techniques of all devices in the architecture.

TABLE II Comparison of 64 point FFT/IFFT PROCESSOR REPORT

Design	Word Length	Gate Counts	Technology	Power
[1]	16	33590	180nm	9.79mW
Ours	16	12604	120nm	1.6184mW

TABLE III AREA AND POWER REPORT ANALYSIS

Description	Transmitter		Receiver	
	Area (nm ²)	Power (mW)	Area (nm ²)	Power (mW)
Hamming Encoding and Decoding	13701.4	2.6393	13392.7	3.6456
Convolutional Encoding and Viterbi Decoding	13421.7	3.3227	14262.7	3.8017
Convolutional Encoding and Sequential Decoding	13421.7	3.3227	13307.9	2.0228

IV. CONCLUSION

The efficient MIMO-OFDM system architecture is described in this work. Considering all the blocks in the architecture were designed especially reconfigurable complex constant multiplier and bit parallel multiplier was designed for pipeline FFT/IFFT block in order to reduce the size of twiddle factor ROM. The result of OFDM architecture shows that the design meets the efficient power, area and timing specifications. Using Synopsys tool the architecture using convolutional encoding and sequential decoding consumes 3.3227mW power for transmitter and 2.0228mW power for receiver section. The transmitter design contains 13421.7 numbers of logic cells and 13307.9 numbers of logic cells for receiver design. From the analysis of coding techniques the result shows that the architecture using convolutional encoding and sequential decoding gives the efficient power and area specifications that improves the performance of the OFDM architecture for fixed WiMAX applications.

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